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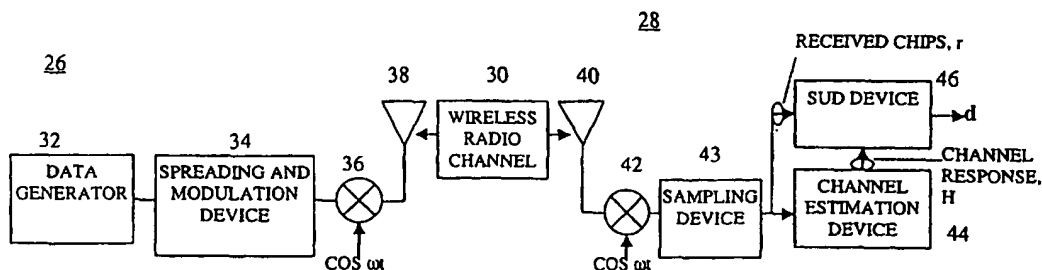
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(54) Title: **SINGLE USER DETECTION**



(57) Abstract: A transmitter site transmit a plurality of data signals over a shared spectrum in a code division multiple access communication system. Each transmitted data signal experiences a similar channel response. A combined signal of the transmitted data signals is received. The combined signal is sampled at a multiple of the chip rate. The channel response for the combined signal is determined. A first element of a spread data vector is determined using the combined signal samples and the estimated channel response. Using a factor from the first element determination, remaining elements of the spread data vector are determined. The data of the data signals is determined using the determined elements of the spread data vector.

[0001] SINGLE USER DETECTION

[0002] BACKGROUND

[0003] This application claims priority to U.S. Provisional Patent Application No. 60/246,947, filed on November 9, 2000.

[0004] The invention generally relates to wireless communication systems. In particular, the invention relates to data detection in a wireless communication system.

[0005] Figure 1 is an illustration of a wireless communication system 10. The communication system 10 has base stations 12_1 to 12_5 (12) which communicate with user equipments (UEs) 14_1 to 14_3 (14). Each base station 12 has an associated operational area, where it communicates with UEs 14 in its operational area.

[0006] In some communication systems, such as code division multiple access (CDMA) and time division duplex using code division multiple access (TDD/CDMA), multiple communications are sent over the same frequency spectrum. These communications are differentiated by their channelization codes. To more efficiently use the frequency spectrum, TDD/CDMA communication systems use repeating frames divided into time slots for communication. A communication sent in such a system will have one or multiple associated codes and time slots assigned to it. The use of one code in one time slot is referred to as a resource unit.

[0007] Since multiple communications may be sent in the same frequency spectrum and at the same time, a receiver in such a system must distinguish between the multiple communications. One approach to detecting such signals is multiuser detection. In multiuser detection, signals associated with all the UEs 14, users, are detected simultaneously. Approaches for implementing multiuser detection include block linear equalization based joint detection (BLE-JD) using a Cholesky or an approximate Cholesky decomposition. These approaches have a high complexity. The high complexity leads to increased power

consumption, which at the UE 14₁ results in reduced battery life. Accordingly, it is desirable to have alternate approaches to detecting received data.

[0008] SUMMARY

[0009] A transmitter site transmits a plurality of data signals over a shared spectrum in a code division multiple access communication system. Each transmitted data signal experiences a similar channel response. A combined signal of the transmitted data signals is received. The combined signal is sampled at a multiple of the chip rate. The common channel response for the received combined signal is estimated. A first element of a spread data vector is determined using the combined signal samples and the estimated channel response. Using a factor from the first element determination, remaining elements of the spread data vector are determined. The data of the data signals is determined using the determined elements of the spread data vector.

[00010] BRIEF DESCRIPTION OF THE DRAWING(S)

[00011] Figure 1 is a wireless communication system.

[00012] Figure 2 is a simplified transmitter and a single user detection receiver.

[00013] Figure 3 is an illustration of a communication burst.

[00014] Figure 4 is a flow chart of an extended forward substitution approach to single user detection (SUD).

[00015] Figure 5 is a flow chart of an approximate banded Cholesky approach to SUD.

[00016] Figure 6 is a flow chart of a Toeplitz approach to SUD.

[00017] Figure 7 is a flow chart of a fast fourier transform (FFT) approach applied to the channel correlation matrix for SUD.

[00018] Figure 8 is a flow chart of a FFT approach to SUD using effective combining.

[00019] Figure 9 is a flow chart of a FFT approach to SUD using zero padding.

[00020] DETAILED DESCRIPTION OF THE PREFERRED EMBODIMENT(S)

[00021] Figure 2 illustrates a simplified transmitter 26 and receiver 28 using single user detection (SUD) in a TDD/CDMA communication system, although the single user detection approaches are applicable to other systems, such as frequency division duplex (FDD) CDMA. In a typical system, a transmitter 26 is in each UE 14 and multiple transmitting circuits 26 sending multiple communications are in each base station 12. The SUD receiver 28 may be at a base station 12, UEs 14 or both. SUD is typically used to detect data in a single or multicode transmission from a particular transmitter. When all the signals are sent from the same transmitter, each of the individual channel code signals in the multicode transmission experience the same channel impulse response. SUD is particularly useful in the downlink, where all transmissions originate from a base station antenna or antenna array. It is also useful in the uplink, where a single user monopolizes a timeslot with a single code or multicode transmission.

[00022] The transmitter 26 sends data over a wireless radio channel 30. A data generator 32 in the transmitter 26 generates data to be communicated to the receiver 28. A modulation/spreading sequence insertion device 34 spreads the data and makes the spread reference data time-multiplexed with a midamble training sequence in the appropriate assigned time slot and codes for spreading the data, producing a communication burst or bursts.

[00023] A typical communication burst 16 has a midamble 20, a guard period 18 and two data bursts 22, 24, as shown in Figure 3. The midamble 20 separates the two data fields 22, 24 and the guard period 18 separates the communication bursts to allow for

the difference in arrival times of bursts transmitted from different transmitters 26. The two data bursts 22, 24 contain the communication burst's data.

[00024] The communication burst(s) are modulated by a modulator 36 to radio frequency (RF). An antenna 38 radiates the RF signal through the wireless radio channel 30 to an antenna 40 of the receiver 28. The type of modulation used for the transmitted communication can be any of those known to those skilled in the art, such as quadrature phase shift keying (QPSK) or M-ary quadrature amplitude modulation (QAM).

[00025] The antenna 40 of the receiver 28 receives various radio frequency signals. The received signals are demodulated by a demodulator 42 to produce a baseband signal. The baseband signal is sampled by a sampling device 43, such as one or multiple analog to digital converters, at the chip rate or a multiple of the chip rate of the transmitted bursts. The samples are processed, such as by a channel estimation device 44 and a SUD device 46, in the time slot and with the appropriate codes assigned to the received bursts. The channel estimation device 44 uses the midamble training sequence component in the baseband samples to provide channel information, such as channel impulse responses. The channel impulse responses can be viewed as a matrix, H . The channel information is used by the SUD device 46 to estimate the transmitted data of the received communication bursts as soft symbols.

[00026] The SUD device 46 uses the channel information provided by the channel estimation device 44 and the known spreading codes used by the transmitter 26 to estimate the data of the desired received communication burst(s). Although SUD is explained using the third generation partnership project (3GPP) universal terrestrial radio access (UTRA) TDD system as the underlying communication system, it is applicable to other systems. That system is a direct sequence wideband CDMA (W-CDMA) system, where the uplink and downlink transmissions are confined to mutually exclusive time slots.

[00027] The receiver 28 receives using its antenna 40 a total of K bursts that arrive simultaneously, 48. The K bursts are superimposed on top of each other in one observation interval. For the 3GPP UTRA TDD system, each data field of a time slot corresponds to one observation interval.

[00028] For one observation interval, the data detection problem is viewed as per Equation 1:

$$r = H \cdot d + n \quad \text{Equation 1}$$

r is the received samples. H is the channel response matrix. d is the spread data vector. The spread data matrix contains the data transmitted in each channel mixed with that channel's spreading code.

[00029] When the received signal is oversampled, multiple samples of each transmitted chip are produced resulting in received vectors, r_1, \dots, r_N , (48). Similarly, the channel estimation device 44 determines the channel responses, H_1, \dots, H_N , corresponding to the received vectors, r_1, \dots, r_N , (50). For twice the chip rate, Equation 1 becomes Equation 2.

$$\begin{bmatrix} r_1 \\ r_2 \end{bmatrix} = \begin{bmatrix} H_1 \\ H_2 \end{bmatrix} \cdot d + n \quad \text{Equation 2}$$

r_1 is the even samples (at the chip rate) and r_2 is the odd samples (offset half a chip from the r_1 samples). H_1 is the channel response for the even samples and H_2 is the channel response for the odd samples.

[00030] Equation 1 becomes Equation 3 for a multiple N of the chip rate.

$$\begin{bmatrix} r_1 \\ r_2 \\ \vdots \\ r_N \end{bmatrix} = \begin{bmatrix} H_1 \\ H_2 \\ \vdots \\ H_N \end{bmatrix} \cdot \mathbf{d} + \mathbf{n} \quad \text{Equation 3}$$

$r_1, r_2 \dots r_N$ are the multiple of the chip rate samples. Each offset by $1/N$ of a chip. $H_1, H_2 \dots H_N$ are the corresponding channel responses. Although the following discussion focuses on a receiver sampling at twice the chip rate, the same approaches are applicable to any multiple of the chip rate.

[00031] For twice the chip rate sampling, matrices H_1 and H_2 are $(N_s + W - 1)$ by N_s in size. N_s is the number of spread chips transmitted in the observation interval and W is the length of the channel impulse response, such as 57 chips in length. Since the received signal has N_s spread chips, the length of r_1 and r_2 is N_s . Equation 2 is rewritten as Equation 4.

$$\begin{bmatrix} r_1(0) \\ r_1(1) \\ | \\ r_1(W-1) \\ r_1(N_s-1) \\ \text{-----} \\ r_2(0) \\ r_2(1) \\ | \\ r_2(W-1) \\ r_2(N_s-1) \end{bmatrix} = \begin{bmatrix} h_1(0) & 0 & 0 & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} \\ h_1(1) & h_1(0) & 0 & \text{--} & & & & \\ | & | & & & & & & \\ h_1(W-1) & h_1(W-2) & \text{--} & \text{--} & h_1(1) & h_1(0) & 0 & 0 \\ | & | & & & | & | & | & | \\ 0 & 0 & \text{--} & h_1(W-1) & h_1(W-2) & \text{--} & h_1(1) & h_1(0) \\ \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} \\ h_2(0) & 0 & 0 & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} \\ h_2(1) & h_2(0) & 0 & \text{--} & & & & \\ | & | & & & & & & \\ h_2(W-1) & h_2(W-2) & \text{--} & \text{--} & h_2(1) & h_2(0) & 0 & 0 \\ | & | & & & | & | & | & | \\ 0 & 0 & \text{--} & h_2(W-1) & h_2(W-2) & \text{--} & h_2(1) & h_2(0) \\ \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} & \text{--} \end{bmatrix} \cdot \mathbf{d} + \mathbf{n}$$

Equation 4

$r_1(i)$, $r_2(i)$, $h_1(i)$ and $h_2(i)$ is the i^{th} element of the corresponding vector matrix \mathbf{r}_1 , \mathbf{r}_2 , \mathbf{H}_1 and \mathbf{H}_2 , respectively.

[00032] One approach to determine the spread data vector is extended forward substitution, which is explained in conjunction with Figure 4. For extended forward substitution, the received data vector is rearranged so that each even sample is followed by its corresponding odd sample. A similar rearrangement is performed on the channel response matrix, as shown in Equation 5a.

$$\begin{bmatrix} r_1(0) \\ r_2(0) \\ r_1(1) \\ r_2(1) \\ | \\ r_1(W-1) \\ r_2(W-1) \\ | \\ r_1(N_s-1) \\ r_2(N_s-1) \end{bmatrix} = \begin{bmatrix} h_1(0) & 0 & 0 & -- \\ h_2(0) & 0 & 0 & -- \\ h_1(1) & h_1(0) & 0 & -- \\ h_2(1) & h_2(0) & 0 & -- \\ | & | & | & -- \\ h_1(W-1) & h_1(W-2) & -- & -- \\ h_2(W-1) & h_2(W-2) & -- & -- \\ | & | & & \\ 0 & 0 & -- & h_1(W-1) & h_1(W-2) & -- & h_1(1) & h_1(0) \\ 0 & 0 & -- & h_2(W-1) & h_2(W-2) & -- & h_2(1) & h_2(0) \end{bmatrix} \cdot \begin{bmatrix} d(0) \\ d(1) \\ | \\ | \\ d(N_s-1) \end{bmatrix} + \mathbf{n}$$

Equation 5a

Similarly, for an N-multiple of the chip rate sampling, Equation 5b is the arrangement.

$$\begin{bmatrix} r_1(0) \\ r_2(0) \\ | \\ r_N(0) \\ r_1(1) \\ r_2(1) \\ | \\ r_N(1) \\ | \\ r_1(N_s-1) \\ r_2(N_s-1) \\ | \\ r_N(N_s-1) \end{bmatrix} = \begin{bmatrix} h_1(0) & 0 & \cdots & 0 & 0 \\ h_2(0) & 0 & \cdots & 0 & 0 \\ | & | & \cdots & | & | \\ h_N(0) & 0 & \cdots & 0 & 0 \\ h_1(1) & h_1(0) & \cdots & 0 & 0 \\ h_2(1) & h_2(0) & \cdots & 0 & 0 \\ | & | & \cdots & | & | \\ h_N(1) & h_N(0) & \cdots & 0 & 0 \\ | & | & \cdots & | & | \\ 0 & 0 & \cdots & h_1(1) & h_1(0) \\ 0 & 0 & \cdots & h_2(1) & h_2(0) \\ | & | & \cdots & | & | \\ 0 & 0 & \cdots & h_N(1) & h_N(0) \end{bmatrix} \cdot \begin{bmatrix} d(0) \\ d(1) \\ | \\ | \\ d(N_s-1) \end{bmatrix} + \mathbf{n}$$

Equation 5b

$d(i)$ is the i^{th} element of the spread data vector, \mathbf{d} . The length of the spread data vector is N_s . Using extended forward substitution, the zero-forcing solution to determine $d(0), \hat{d}(0)$, is per Equations 6a and 7a, (52).

$$\begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \cdot d(0) = \begin{bmatrix} r_1(0) \\ r_2(0) \end{bmatrix} \quad \text{Equation 6a}$$

$$\hat{d}(0) = \left\{ \begin{bmatrix} h_1(0) & h_2(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \right\}^{-1} \begin{bmatrix} h_1(0) & h_2(0) \end{bmatrix} \begin{bmatrix} r_1(0) \\ r_2(0) \end{bmatrix} \quad \text{Equation 7a}$$

Equation 6a is the general formula for $d(0)$. Equation 7a is the zero forcing solution for $\hat{d}(0)$. Similarly, for N-multiple of the chip rate, Equations 6b and 7b are used.

$$\begin{bmatrix} h_1(0) \\ h_2(0) \\ | \\ h_N(0) \end{bmatrix} d(0) = \begin{bmatrix} r_1(0) \\ r_2(0) \\ | \\ r_N(0) \end{bmatrix} \quad \text{Equation 6b}$$

$$\hat{d}(0) = \left\{ \begin{bmatrix} h_1(0) \\ h_2(0) \\ \vdots \\ h_N(0) \end{bmatrix} \right\}^{-1} \begin{bmatrix} h_1(0) & \dots & h_N(0) \end{bmatrix} \begin{bmatrix} r_1(0) \\ r_2(0) \\ \vdots \\ r_N(0) \end{bmatrix} \quad \text{Equation 7b}$$

In solving Equation 7a and 7b, for later use \mathbf{v}^H is determined as illustrated by Equation 8 for the \mathbf{v}^H for Equation 7a and stored, (52).

$$\mathbf{v}^H = \left\{ \begin{bmatrix} h_1(0) & h_2(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \right\}^{-1} \begin{bmatrix} h_1(0) & h_2(0) \end{bmatrix} \quad \text{Equation 8}$$

$\hat{d}(0)$ is determined using \mathbf{v}^H per Equation 9.

$$\hat{d}(0) = \mathbf{v}^H \begin{bmatrix} r_1(0) \\ r_2(0) \end{bmatrix} \quad \text{Equation 9}$$

Using the Toplitz structure of the H matrix, the remaining spread data elements can be determined sequentially using zero forcing per Equation 10a, (54).

$$\hat{d}(i) = \mathbf{v}^H \left\{ \begin{bmatrix} r_1(i) \\ r_2(i) \end{bmatrix} - \begin{bmatrix} h_1(i) \\ h_2(i) \end{bmatrix} \hat{d}(0) + \sum_{j=1}^{i-1} \begin{bmatrix} h_1(j) \\ h_2(j) \end{bmatrix} \hat{d}(i-j-1) \right\} \quad \text{Equation 10a}$$

For an N-multiple of the chip rate, Equation 10b is used.

$$\hat{d}(i) = \mathbf{v}^H \left\{ \begin{bmatrix} r_1(i) \\ | \\ r_N(i) \end{bmatrix} - \begin{bmatrix} h_1(i) \\ | \\ h_N(i) \end{bmatrix} \hat{d}(0) - \sum_{j=1}^{i-1} \begin{bmatrix} h_1(j) \\ | \\ h_N(j) \end{bmatrix} \cdot \hat{d}(i-j-1) \right\} \quad \text{Equation 10b}$$

After the spread data vector is determined, each communication burst's data is determined by despreading, such as by mixing the spread data vector with each burst's code, (56).

[00033] The complexity in using the extended forward substitution approach, excluding despreading, is summarized in Table 1.

Calculating \mathbf{v}^H	4 multiplications & 1 reciprocal
Calculating $\hat{d}(0)$	2 multiplications
Calculating $\hat{d}(1)$	4 multiplications
Calculating each up to $\hat{d}(W-1)$	2 multiplications
Calculating each $\hat{d}(i)$ from $\hat{d}(w)$ to $\hat{d}(N_s-1)$	$2W + 2$ multiplications
Total Number of Multiplications	$2N_s + (W-1) \cdot W + 2W \cdot (N_s - W + 1)$
Total Number of Calculations	$2N_s + (W-1) \cdot W + 2W \cdot (N_s - W + 1) + 5$

Table 1

[00034] For a TDD burst type II, N_s is 1104 and W is 57, solving for d using extended forward substitution 200 times per second requires 99.9016 million real

operations per second (MROPS) for twice the chip rate sampling or 49.95 MROPS for chip rate sampling.

[00035] Another approach to estimate data is an approximate banded Cholesky approach, which is explained in conjunction with Figure 5. A cross correlation matrix R is determined so that it is square, (N_s by N_s), and banded per Equation 11, (58).

$$R = H^H H \quad \text{Equation 11}$$

$(\cdot)^H$ indicates the hermetian function. H is of size $2(N_s + W - 1)$ by N_s . Equation 11 is rewritten as Equation 12a for twice the chip rate sampling.

$$R = \begin{bmatrix} H_1^H & H_2^H \end{bmatrix} \cdot \begin{bmatrix} H1 \\ H2 \end{bmatrix} = H_1^H H_1 + H_2^H H_2 \quad \text{Equation 12a}$$

For an N-multiple of the chip rate, Equation 12b is used.

$$R = \begin{bmatrix} H_1^H & H_2^H & \dots & H_N^H \end{bmatrix} \begin{bmatrix} H_1 \\ H_2 \\ | \\ H_N \end{bmatrix} \quad \text{or} \quad \text{Equation 12b}$$

$$R = \sum_{i=1}^N H_i^H H_i$$

[00036] Using Equation 12a or 12b, the resulting R is of size N_s by N_s and banded as illustrated in Equation 13 for twice the chip rate sampling, $W = 3$ and $N_s = 10$.

$$R = \begin{bmatrix} R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 & 0 & 0 \\ R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 & 0 \\ R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 \\ 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 \\ 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 \\ 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 \\ 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 \\ 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 \\ 0 & 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 \\ 0 & 0 & 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 \end{bmatrix} \quad \text{Equation 13}$$

[00037] In general, the bandwidth of R is per Equation 14.

$$p = W - 1 \quad \text{Equation 14}$$

[00038] Using an approximate Cholesky approach, a sub-block of R, R_{sub} , of size N_{col} by N_{col} is used. A typical size of R_{sub} is $2W - 1$ by $2W - 1$, although other sized matrices may be used. The sub-block, R_{sub} , is decomposed using Cholesky decomposition per Equation 15, (60):

$$R_{\text{sub}} = G G^H \quad \text{Equation 15}$$

[00039] The Cholesky factor G is of size N_{col} by N_{col} . An illustration of a 5×5 G matrix with $W = 3$ is per Equation 16.

$$G = \begin{bmatrix} G_{11} & 0 & 0 & 0 & 0 \\ G_{21} & G_{22} & 0 & 0 & 0 \\ G_{31} & G_{32} & G_{33} & 0 & 0 \\ 0 & G_{42} & G_{43} & G_{44} & 0 \\ 0 & 0 & G_{53} & G_{54} & G_{55} \end{bmatrix} \quad \text{Equation 16}$$

G_{ij} is the element of the G matrix at the i^{th} column and j^{th} row. The G matrix is extended to an N_s by N_s matrix, G_{full} , by right shifting the bottom row of G by one element for each row after the last row of G , (62). For $N_s = 10$, the illustration of Equation 16 is expanded per Equation 17, (62).

$$G_{\text{full}} = \begin{bmatrix} G_{11} & 0 & & & & & & & & \\ G_{21} & G_{22} & 0 & & & & & & & \\ G_{31} & G_{32} & G_{33} & 0 & & & & & & \\ 0 & G_{42} & G_{43} & G_{44} & 0 & & & & & \\ & 0 & G_{53} & G_{54} & G_{55} & 0 & & & & \\ & & 0 & G_{53} & G_{54} & G_{55} & 0 & & & \\ & & & 0 & G_{53} & G_{54} & G_{55} & 0 & & \\ & & & & 0 & G_{53} & G_{54} & G_{55} & 0 & \\ & & & & & 0 & G_{53} & G_{54} & G_{55} & 0 \\ & & & & & & 0 & G_{53} & G_{54} & G_{55} \end{bmatrix}$$

Equation 17

[00040] The spread data vector is determined using forward and backward substitution, (64). Forward substitution is used to determine y per Equation 18a for twice the chip rate sampling and Equation 18b for a multiple N of the chip rate sampling.

$$G_{\text{full}}y = H_1^H r_1 + H_2^H r_2 \quad \text{Equation 18a}$$

$$G_{\text{full}}y = H_1^H r_1 + H_2^H r_2 + \dots + H_N^H r_N \quad \text{Equation 18b}$$

Backward substitution is subsequently used to solve for the spread data vector per Equation 19.

$$G_{full}^H \mathbf{d} = \mathbf{y}$$

Equation 19

[00041] After the spread data vector, \mathbf{d} , is determined, each burst's data is determined by despreading, (66).

[00042] The complexity of approximate Cholesky decomposition, excluding despreading, for twice the chip rate sampling is per Table 2.

Operation	Number of Calculations
Calculating $H^H H$	$W(W+1)$
Calculating Cholesky Decomposition	$\frac{N_{col}(W-1)^2}{2} + \frac{3N_{col}(W-1)}{2} - \frac{(W-1)^3}{3} - (W-1)^2 - \frac{2(W-1)}{3}$
Calculating $H^H \mathbf{r}$	$2N_s W$
Forward Substitution	$\left[N_s - \frac{(W-1)}{2} \right] W$ and the reciprocal of N_s real numbers
Backward Substitution	$\left[N_s - \frac{(W-1)}{2} \right] W$ and the reciprocal of N_s real numbers

Table 2

[00043] For a TDD burst type II, N_s is 1104 and for W is 57, performing approximate banded Cholesky 200 times per second at twice the chip rate requires

272.56 MROPS. By contrast, an exact banded Cholesky approach requires 906.92 MROPS. For chip rate sampling, the approximate banded Cholesky approach requires 221.5 MROPS.

[00044] Another approach for data detection uses a Toeplitz approach, (Levinson-Durbin type algorithm), which is explained in conjunction with Figure 6. The R matrix of Equation 12a and 12b is reproduced here.

$$R = \begin{bmatrix} H_1^H & H_2^H \end{bmatrix} \cdot \begin{bmatrix} H1 \\ H2 \end{bmatrix} = H_1^H H_1 + H_2^H H_2 \quad \text{Equation 12a}$$

For an N-multiple of the chip rate, Equation 12b is used.

$$R = \begin{bmatrix} H_1^H & H_2^H & \dots & H_N^H \end{bmatrix} \begin{bmatrix} H_1 \\ H_2 \\ | \\ H_N \end{bmatrix} \quad \text{or} \quad \text{Equation 12b}$$

$$R = \sum_{i=1}^N H_i^H H_i$$

[00045] The R matrix is symmetric and Toeplitz with a bandwidth of $p = W - 1$, (68). A left most upper corner of the R matrix, $R(k)$, being a k by k matrix is determined as shown in Equation 20.

$$R(k) = \begin{bmatrix} R_0 & R_1 & \dots & R_{k-1} \\ R_1 & R_0 & & \vdots \\ & & \ddots & \\ R_{k-1} & R_{k-2} & \dots & R_0 \end{bmatrix} \quad \text{Equation 20}$$

Additionally, another vector R_k is determined using elements of R, per Equation 21, (72).

$$\mathbf{R}_k = \begin{bmatrix} R_1 \\ R_2 \\ \vdots \\ R_k \end{bmatrix}. \quad \text{Equation 21}$$

Bolding indicates a matrix including all elements up to its subscript. At stage $k + 1$, the system is solved per Equation 22.

$$\mathbf{R}(k+1)\mathbf{d}(k+1) = [\mathbf{H}^H \mathbf{r}]_{k+1} \quad \text{Equation 22}$$

$[\mathbf{H}^H \mathbf{r}]_{k+1}$ is the first $(k + 1)$ components of $\mathbf{H}^H \mathbf{r}$. $\mathbf{d}(k+1)$ is broken into a vector $\mathbf{d}_1(k+1)$ of length k and a scalar $d_2(k+1)$ as per Equation 23.

$$\mathbf{d}(k+1) = \begin{bmatrix} \mathbf{d}_1(k+1) \\ d_2(k+1) \end{bmatrix}. \quad \text{Equation 23}$$

[00046] The matrix $\mathbf{R}(k+1)$ is decomposed as per Equation 24.

$$\mathbf{R}(k+1) = \begin{bmatrix} \mathbf{R}(k) & \vdots & \mathbf{E}_k \mathbf{R}_k \\ \cdots & \vdots & \cdots \\ \mathbf{R}_k^H \mathbf{E}_k & \vdots & R_0 \end{bmatrix}. \quad \text{Equation 24}$$

[00047] \mathbf{E}_k is an exchange matrix. The exchange matrix operates on a vector by reversing that vectors elements.

[00048] Using the Yule-Walker equation for linear prediction, Equation 25 results, (78).

$$\begin{bmatrix} R(k-1) & \vdots & E_{k-1} \mathbf{R}_{k-1} \\ \dots & \vdots & \dots \\ \mathbf{R}_{k-1}^H E_{k-1} & \vdots & R_0 \end{bmatrix} \begin{bmatrix} y_1(k) \\ y_2(k) \end{bmatrix} = - \begin{bmatrix} \mathbf{R}_{k-1} \\ R_k \end{bmatrix} \quad \text{Equation 25}$$

[00049] Using order recursions, Equations 26, 27 and 28 result.

$$y_1(k) = y(k-1) + y_2(k) E_{k-1} y(k-1) \quad \text{Equation 26}$$

$$y_2(k) = - \frac{[R_k + \mathbf{R}_{k-1}^H E_{k-1} y(k-1)]}{[1 + \mathbf{R}_{k-1}^H y(k-1)]} \quad \text{Equation 27}$$

$$\mathbf{y}(k) = \begin{bmatrix} y_1(k) \\ y_2(k) \end{bmatrix} \quad \text{Equation 28}$$

[00050] Using $\mathbf{y}(k)$, $\mathbf{d}(k+1)$ is determined per Equations 29, 30 and 31, (74).

$$\mathbf{d}_1(k+1) = \mathbf{d}(k) + d_2(k+1) E_k \mathbf{y}(k) \quad \text{Equation 29}$$

$$d_2(k+1) = \left[\frac{(H^H \mathbf{r})_{k+1} - \mathbf{R}_k^H E_k \mathbf{d}(k)}{1 + \mathbf{R}_k^H \mathbf{y}(k)} \right] \quad \text{Equation 30}$$

$$\mathbf{d}(k+1) = \begin{bmatrix} \mathbf{d}_1(k+1) \\ d_2(k+1) \end{bmatrix} \quad \text{Equation 31}$$

$(H^H \mathbf{r})_{k+1}$ is the $(k+1)^{\text{th}}$ element of $H^H \mathbf{r}$.

[00051] After properly initializing the recursions, the recursions are computed for $k = 1, 2, \dots, N_S$. $\mathbf{d}(N_S)$ is a solution to Equation 32, (74).

$$R\mathbf{d} = H^H \mathbf{r} \quad \text{Equation 32}$$

[00052] The spread data vector \mathbf{d} is despread with the bursts' channelization codes to recover the data, (76).

[00053] The banded structure of R affects the recursions as follows. $R(2)$ and \mathbf{R}_2 are per Equation 33.

$$R(2) = \begin{bmatrix} R_0 & R_1 \\ R_1 & R_0 \end{bmatrix}, \mathbf{R}_2 = \begin{bmatrix} R_1 \\ R_2 \end{bmatrix} \quad \text{Equation 33}$$

[00054] The inner product calculations in Equations 27 and 30 require two multiplications each. To illustrate, the R matrix of Equation 20 for $k = 6$ is per Equation 34.

$$R(6) = \begin{bmatrix} R_0 & R_1 & R_2 & 0 & 0 & 0 \\ R_1 & & & R_2 & 0 & 0 \\ R_2 & & & & R_2 & 0 \\ 0 & R_2 & & & & R_2 \\ 0 & 0 & R_2 & & & R_1 \\ 0 & 0 & 0 & R_2 & & R_0 \end{bmatrix}, \mathbf{R}_6 = \begin{bmatrix} R_1 \\ R_2 \\ 0 \\ 0 \\ 0 \\ 0 \end{bmatrix} \quad \text{Equation 34}$$

[00055] The number of non-zero elements in the vector \mathbf{R}_6 is equal to the bandwidth, p , of the matrix R . When the inner product of $\mathbf{R}_6^H E_6 \mathbf{y}(k)$ in Equation 27 and the inner product $\mathbf{R}_6^H E_6 \mathbf{d}(k)$ in Equation 30 are calculated, only p (and not k) multiplications are required. For the recursions of Equations 26 and 29, no computational reductions are obtained.

[00056] Table 3 shows the complexity in implementing the Toeplitz approach.

Calculation	# of Calculations	MROPS
Functions Executed Once Per Burst Calculating $H^H H$		1.3224
Solving Yule-Walker for y	$672,888 \times \frac{100}{10^6}$	269.1552
Functions Executed Twice Per Burst Calculating $H^H r$		100.68
Solving $R(k+1)d(k+1)H^H r$	$672,888 \times \frac{200}{10^6}$	538.3104

Table 3

The total MROPs for the Toeplitz approach for a TDD burst type is 909.4656 MROPs for twice the chip rate sampling and 858.4668 MROPs for chip rate sampling.

[00057] Another approach for data detection uses fast fourier transforms (FFTs), which is explained using Figure 7. If chip rate sampling is used, the channel matrix H is square except for edge effects. Using a circulant approximation for the H matrix, a FFT of the received vector, r , and the channel vector, H , to obtain the data estimate is used.

[00058] For a multiple of the chip rate sampling, such as twice the chip rate, the H matrix is not square or circulant. However, a submatrix, shown by dotted lines, of the channel correlation matrix $R = H^H H$ matrix of Equation 13, (84), as shown for Equation 35a is circulant.

$$R = \begin{bmatrix} R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 & 0 & 0 \\ R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 & 0 \\ \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots \\ R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 & 0 \\ 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 & 0 \\ 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 & 0 \\ 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 & 0 \\ 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 & 0 \\ 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 & R_2 \\ \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots & \dots \\ 0 & 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 & R_1 \\ 0 & 0 & 0 & 0 & 0 & 0 & 0 & R_2 & R_1 & R_0 \end{bmatrix}$$

Equation 35a

For an N-multiple of the chip rate sampling, the channel correlation matrix is determined per Equation 35b.

$$R = \begin{bmatrix} H_1^H H_2^H & \dots & H_N^H \end{bmatrix} \begin{bmatrix} H_1 \\ H_2 \\ \vdots \\ H_N \end{bmatrix} = \sum_{i=1}^N H_i^H H_i$$

Equation 35b

[00059] By approximating the R matrix as being circulant, Equations 36, 37 and 38 are used.

$$R^H = D \Delta D^H$$

Equation 36

$$\Delta = \text{diag}(D(R)_1)$$

$$\hat{d} = \text{diag} \left(D \begin{bmatrix} R_0 \\ R_1 \\ R_2 \\ 0 \\ \vdots \\ 0 \end{bmatrix} \right) \quad \text{Equation 37}$$

$(R)_1$ is the first column of the R matrix expanded to a diagonal matrix. Although described using the first column, this approach can be modified to use any column of the R matrix, (86). However, it is preferred to use a column having the most non-zero elements of any column, such as R_2, R_1, R_0, R_1, R_2 . These columns are typically any column at least W columns from both sides, such as any column between and including W and $N_s - W - 1$. Equations 38 and 39 are used in a zero-forcing equalization approach.

$$R\hat{d} = H^H r \quad \text{Equation 38}$$

$$\hat{d} = R^{-1}(H^H r) \quad \text{Equation 39}$$

[00060] Since D is an orthogonal discrete fourier transform (DFT) matrix, Equations 40, 41 and 42 result.

$$D^H D = N_s I \quad \text{Equation 40}$$

$$D^{-1} = (1/N_s) D^H \quad \text{Equation 41}$$

$$R^{-1} = \frac{1}{N_s} D^H \Delta^{-1} \frac{1}{N_s} D \quad \text{Equation 42}$$

Accordingly, \hat{d} can be determined using a fourier transform per Equations 43, 44 and 45a.

$$R^{-1} = \frac{1}{N_s^2} D^H \Delta^{-1} [D(H^H r)] \quad \text{Equation 43}$$

$$D^H \hat{d} = \frac{1}{N_s} \Delta^{-1} [F(H^H r)] \quad \text{Equation 44}$$

$$F(\hat{d}) = \frac{F(H^H r)}{N_s F((R)_1)} \quad \text{Equation 45a}$$

$(\cdot)_1$ is the first column, although an analogous equation can be used for any column of R . $F(\cdot)$ denotes a fourier transform function. $F(H^H r)$ is preferably calculated using FFTs per Equation 45b.

$$F(H^H r) = N_c [F(h_1)F(r_1) + \dots + F(h_N)F(r_N)] \quad \text{Equation 45b}$$

Taking the inverse fourier transform $F^{-1}(\cdot)$, of the result of Equation 45a produces the spread data vector, (88). The transmitted data can be recovered by despreading using the appropriate codes, (90).

[00061] The complexity of this FFT approach is shown in Table 4.

Functions Executed Once Per Burst Calculation	# of Calculations	MROPs
Calculating $H^H H$		1.3224
$F([R]_1) \cdot N_s \log_2 N_s$	$11160 \times \frac{100}{10^6}$	4.4640
Functions Executed Twice Per Burst Calculating $H^H r$ by FFT		38
Calculating Equation 45		0.8832
$F^{-1}(d) \cdot N_s \log_2 N_s$		8.9280
Total		55 MROPS

Table 4

[00062] The FFT approach is less complex than the other approaches. However, a performance degradation results from the circulant approximation.

[00063] Another approach to use FFTs to solve for the data vector for a multiple of the chip rate sampling combines the samples by weighing, as explained using Figure 8. To illustrate for twice the chip rate sampling, r_1 is the even and r_2 is the odd samples. Each element of r_1 , such as a first element $r_1(0)$, is weighted and combined with a corresponding element of r_2 , such as $r_2(0)$ per Equation 46.

$$r_{eff}(0) = W_1 r_1(0) + W_2 r_2(0)$$

Equation 46

$r_{\text{eff}}(0)$ is the effectively combined element of an effectively combined matrix, r_{eff} . W_1 and W_2 are weights. For N-times the chip rate sampling, Equation 47 is used.

$$r_{\text{eff}}(0) = W_1 r_1(0) + \dots + W_n r_n(0) \quad \text{Equation 47}$$

Analogous weighting of the channel response matrices, H_1 to H_n , is performed to produce H_{eff} , (92). As a result, Equation 3 becomes Equation 48.

$$r_{\text{eff}} = H_{\text{eff}} \mathbf{d} + \mathbf{n} \quad \text{Equation 48}$$

The resulting system is an N_s by N_s system of equations readily solvable by FFTs per Equation 49, (94).

$$F(\mathbf{d}) = \frac{F(r_{\text{eff}})}{F((H_{\text{eff}})_1)} \quad \text{Equation 49}$$

[00064] Using the inverse fourier transform, the spread data vector is determined. The bursts' data is determined by despreding the spread data vector using the bursts' code, (96). Although Equation 49 uses the first column of H_{eff} , the approach can be modified to use any representative column of, H_{eff} .

[00065] Another approach using FFTs uses zero padding, which is explained using Figure 9. Equation 5 is modified by zero padding the data vector so that every other element, such as the even elements are zero, (98). The modified \mathbf{d} matrix is \mathbf{d}^{\sim} . The H matrix is also expanded to form H^{\sim} . H matrix is expanded by repeating each column to the right of that column and shifting each element down one row and zero padding the top of the shifted column. An illustration of such a system for twice the chip rate sampling, $W = 3$ and $N_s = 4$ is per Equation 49a.

$$\begin{bmatrix} r_1(0) \\ r_2(0) \\ r_1(1) \\ r_2(1) \\ r_1(2) \\ r_2(2) \\ r_1(3) \\ r_2(3) \end{bmatrix} = \begin{bmatrix} h_1(0) & & & & & & & \\ h_2(0) & h_1(0) & & & & & & \\ h_1(1) & h_2(0) & h_1(0) & & & & & \\ h_2(1) & h_1(1) & h_2(0) & h_1(0) & & & & \\ h_1(2) & h_2(1) & h_1(1) & h_2(0) & h_1(0) & h_2(0) & & \\ h_2(2) & h_1(2) & h_2(1) & h_1(1) & h_2(0) & h_1(0) & h_2(0) & \\ 0 & h_2(2) & h_1(2) & h_2(1) & h_1(1) & h_2(0) & h_1(0) & h_2(0) \\ 0 & 0 & h_2(2) & h_1(2) & h_2(1) & h_1(1) & h_2(0) & h_1(0) \end{bmatrix} \cdot \begin{bmatrix} d(0) \\ 0 \\ d(1) \\ 0 \\ d(2) \\ 0 \\ d(3) \\ 0 \end{bmatrix} + \mathbf{n}$$

Equation 49a

For an N-multiple of the chip rate, Equation 49b is used as shown for simplicity for $N_s = 3$.

$$\begin{bmatrix} r_1(0) \\ r_2(0) \\ | \\ r_N(0) \\ r_1(1) \\ r_2(1) \\ | \\ r_N(1) \\ r_1(2) \\ r_2(2) \\ | \\ r_{N-1}(2) \\ r_N(2) \end{bmatrix} = \begin{bmatrix} h_1(0) & 0 & -- & 0 \\ h_2(0) & h_1(0) & -- & 0 \\ | & | & -- & | \\ h_N(0) & h_{N-1}(0) & -- & 0 \\ h_1(1) & h_N(0) & -- & 0 \\ h_2(1) & h_1(1) & -- & 0 \\ | & | & -- & | \\ h_N(1) & h_{N-1}(1) & -- & 0 \\ 0 & h_N(1) & -- & 0 \\ 0 & 0 & -- & 0 \\ | & | & -- & | \\ 0 & 0 & -- & h_2(0) \\ 0 & 0 & -- & h_1(0) \end{bmatrix} \cdot \begin{bmatrix} d(0) \\ 0 \\ | \\ 0 \\ d(1) \\ 0 \\ | \\ 0 \\ d(2) \\ 0 \\ | \\ 0 \end{bmatrix} + \mathbf{n}$$

Equation 49b

In general, the H^\sim matrix for an N multiple is $(N N_s)$ by $(N N_s)$. The matrix H^\sim is square, Toeplitz and approximately circulant and is of size $2N_s$ by $2N_s$. The zero forcing solution is per Equation 50, (100).

$$F(\mathbf{d}^\sim) = \frac{F(\mathbf{r})}{F((H^\sim)_1)} \quad \text{Equation 50}$$

[00066] A column other than the first column may be used in an analogous FFT. Furthermore, since any column may be used, a column from the original channel response matrix, H or an estimated expanded column of the H^\sim derived from a column of H. Using every N^{th} value from \mathbf{d}^\sim , \mathbf{d} is estimated. Using the appropriate codes, \mathbf{d} is despread to recover the data, (102).

* * *

CLAIMS

What is claimed is:

1. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

estimating a channel response for the combined signal at the multiple of the chip rate;

determining a first element of a spread data vector using the combined signal samples and the estimated channel response;

using a factor from the first element determination to determine remaining elements of the spread data vector; and

estimating data of the data signals using the determined elements of the spread data vector.

2. The method of claim 1 wherein the factor is derived using the channel response.

3. The method of claim 1 wherein the multiple of the chip rate is N-multiple of the chip rate and the factor is \mathbf{v}^H and a first element of each channel response matrix corresponding to each N-multiple of the chip rate is $h_1(0), h_2(0) \dots h_N(0)$ and

$$v^H = \left\{ \begin{bmatrix} h_1(0) & \dots & h_N(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ \vdots \\ h_N(0) \end{bmatrix} \right\}^{-1} [h_1(0) \dots h_N(0)].$$

4. The method of claim 3 wherein N is 2 and

$$v^H = \left\{ \begin{bmatrix} h_1(0)h_2(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \right\}^{-1} [h_1(0)h_2(0)].$$

5. The method of claim 3 wherein an i^{th} element of the spread data vector, $\hat{d}(i)$, other than the first element is determined per

$$\hat{d}(i) = v^H \left\{ \begin{bmatrix} r_1(i) \\ | \\ r_N(i) \end{bmatrix} - \begin{bmatrix} h_1(i) \\ | \\ h_N(i) \end{bmatrix} \hat{d}(0) - \sum_{j=1}^{i-1} \begin{bmatrix} h_1(j) \\ | \\ h_N(j) \end{bmatrix} \cdot d(i-j-1) \right\}.$$

6. The method of claim 1 wherein the data estimating is by despreading the spread data vector.

7. The method of claim 1 wherein the factor is stored prior to the remaining elements determination.

8. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the

transmitted data signals;

means for estimating a channel response for the combined signal at the multiple of the chip rate;

means for determining a first element of a spread data vector using the combined signal samples and the estimated channel response;

means for using a factor from the first element determination to determine remaining elements of the spread data vector; and

means for estimating data of the data signals using the determined elements of the spread data vector.

9. The receiver of claim 8 wherein the factor is derived using the channel response.

10. The receiver of claim 8 wherein the multiple of the chip rate is N-multiple of the chip rate and the factor is \mathbf{v}^H and a first element of each channel response matrix corresponding to each N-multiple of the chip rate is $h_1(0), h_2(0) \dots h_N(0)$ and

$$\mathbf{v}^H = \left\{ \begin{bmatrix} h_1(0) \\ h_1(0) \dots h_N(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ \vdots \\ h_N(0) \end{bmatrix} \right\}^{-1} [h_1(0) \dots h_N(0)].$$

11. The receiver of claim 10 wherein N is 2 and

$$\mathbf{v}^H = \left\{ \begin{bmatrix} h_1(0)h_2(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \right\}^{-1} [h_1(0)h_2(0)].$$

12. The receiver of claim 8 wherein the data estimating is by despreading the spread data vector.

13. The receiver of claim 8 wherein the factor is stored prior to the remaining elements determination.

14. The code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response for the combined signal at the multiple of the chip rate; and

a single user detection device for determining a first element of a spread data vector using the combined signal samples and the estimated channel response and for using a factor from the first element determination to determine remaining elements of the spread data vector;

wherein data of the data signals is estimated from the spread data vector.

15. The receiver of claim 14 wherein the factor is derived using the channel response.

16. The receiver of claim 14 wherein the multiple of the chip rate is N-multiple of the chip rate and the factor is \mathbf{v}^H and a first element of each channel response matrix corresponding to each N-multiple of the chip rate is $h_1(0), h_2(0) \dots h_N(0)$ and

$$\mathbf{v}^H = \left\{ \begin{bmatrix} h_1(0) & \dots & h_N(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ \vdots \\ h_N(0) \end{bmatrix} \right\}^{-1} [h_1(0) \dots h_N(0)].$$

17. The receiver of claim 16 wherein N is 2 and

$$\mathbf{v}^H = \left\{ \begin{bmatrix} h_1(0)h_2(0) \end{bmatrix} \begin{bmatrix} h_1(0) \\ h_2(0) \end{bmatrix} \right\}^{-1} [h_1(0)h_2(0)].$$

18. The receiver of claim 14 wherein the data estimating is by despreading the spread data vector.

19. The receiver of claim 14 wherein the factor is stored prior to the remaining elements determination.

20. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the data signals;
estimating a channel response for the combined signal at the multiple of the chip rate;

determining a cross correlation matrix using the estimated channel response;

selecting a subblock of the cross correlation matrix;

determining a Cholesky factor for the subblock;

extending the Cholesky factor;

determining the spread data vector using the extended Cholesky factor, a

version of the channel response and the samples;

estimating data of the data signals using the spread data vector.

21. The method of claim 20 wherein the channel response is estimated as a channel response matrix and the cross correlation matrix is the hermetian of the channel response matrix multiplied by the channel response matrix.

22. The method of claim 21 wherein the multiple is twice the chip rate sampling, the channel response matrix has even matrix samples H_1 and odd matrix samples H_2 .

23. The method of claim 21 wherein the multiple is N -times the chip rate sampling, the channel response matrix has N sets of matrix samples, $H_1, H_2, \dots H_N$.

24. The method of claim 20 wherein the subblock has $2W - 1$ by $2W - 1$ elements of the cross correlation matrix and W is a length of the impulse response.

25. The method of claim 20 wherein the determining the spread data vector uses forward and backward substitution.

26. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the data signals;

means for estimating a channel response for the combined signal at the multiple of the chip rate;

means for determining a cross correlation matrix using the estimated channel response;

means for selecting a subblock of the cross correlation matrix;

means for determining a Cholesky factor for the subblock;

means for extending the Cholesky factor;

means for determining the spread data vector using the extended Cholesky factor, a version of the channel response and the samples; and

means for estimating data of the data signals using the spread data vector.

27. The receiver of claim 26 wherein the channel response is estimated as a channel response matrix and the cross correlation matrix is the hermetian of the channel response matrix multiplied by the channel response matrix.

28. The receiver of claim 27 wherein the multiple is twice the chip rate sampling, the channel response matrix has even matrix samples H_1 and odd matrix samples H_2 .

29. The receiver of claim 27 wherein the multiple is N-times the chip rate sampling, the channel response matrix has N sets of matrix samples, $H_1, H_2, \dots H_N$.

30. The receiver of claim 26 wherein the subblock has $2W - 1$ by $2W - 1$ elements of the cross correlation matrix and W is a length of the impulse response.

31. The receiver of claim 26 wherein the determining the spread data vector uses forward and backward substitution.

32. A code division multiple access receiver for use in receiving a plurality

of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response for the combined signal at the multiple of the chip rate; and

a single user detection device for determining a cross correlation matrix using the estimated channel response, for selecting a subblock of the cross correlation matrix, for determining a Cholesky factor for the subblock, for extending the Cholesky factor and for determining the spread data vector using the extended Cholesky factor, a version of the channel response and the samples; and

wherein data of the data signals is estimated from the spread data vector.

33. The receiver of claim 32 wherein the channel response is estimated as a channel response matrix and the cross correlation matrix is the hermetian of the channel response matrix multiplied by the channel response matrix.

34. The receiver of claim 33 wherein the multiple is twice the chip rate sampling, the channel response matrix has even matrix samples H_1 and odd matrix samples H_2 .

35. The receiver of claim 33 wherein the multiple is N-times the chip rate sampling, the channel response matrix has N sets of matrix samples, $H_1, H_2, \dots H_N$.

36. The receiver of claim 32 wherein the subblock has $2W - 1$ by $2W - 1$

elements of the cross correlation matrix and W is a length of the impulse response.

37. The receiver of claim 32 wherein the determining the spread data vector uses forward and backward substitution.

38. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the combined signal;

estimating a channel response for the combined signal at the multiple of the chip rate;

determining a cross correlation matrix using the estimated channel response;

determining the spread data vector using order recursions by determining a first spread data estimate using an element from the cross correlation matrix and recursively determining further estimates using additional elements of the cross correlation matrix; and

estimating data of the data signals using the spread data vector.

39. The method of claim 38 wherein the spread data estimates are determined by combining a scalar and a vector portions of the spread data estimates.

40. The method of claim 38 wherein the spread data vector determining is performed using Yule-Walker equations.

41. The method of claim 38 wherein the first spread data estimate is determined using an element of an upper left corner of the cross correlation matrix.

42. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the combined signal;

means for estimating a channel response for the combined signal at the multiple of the chip rate;

means for determining a cross correlation matrix using the estimated channel response;

means for determining the spread data vector using order recursions by determining a first spread data estimate using an element from the cross correlation matrix and recursively determining further estimates using additional elements of the cross correlation matrix; and

means for estimating data of the data signals using the spread data vector.

43. The receiver of claim 42 wherein the spread data estimates are determined by combining a scalar and a vector portions of the spread data estimates.

44. The receiver of claim 42 wherein the spread data vector determining is performed using Yule-Walker equations.

45. The receiver of claim 42 wherein the first spread data estimate is

determined using an element of an upper left corner of the cross correlation matrix.

46. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response for the combined signal at the multiple of the chip rate; and

a single user detection device for determining a cross correlation matrix using the estimated channel responses, for determining the spread data vector using order recursions by determining a first spread data estimate using an element from the cross correlation matrix and recursively determining further estimates using additional elements of the cross correlation matrix; and

wherein data of the data signals is estimated from the spread data vector.

47. The receiver of claim 46 wherein the spread data estimates are determined by combining a scalar and a vector portions of the spread data estimates.

48. The receiver of claim 46 wherein the spread data vector determining is performed using Yule-Walker equations.

49. The receiver of claim 46 wherein the first spread data estimate is determined using an element of an upper left corner of the cross correlation matrix.

50. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the combined signal;

estimating a channel response for the combined signal at the multiple of the chip rate;

determining a column of a channel correlation matrix using the estimated channel response;

determining a spread data vector using the determined column, the estimated channel response, the received combined signal and a fourier transform; and

estimating data of the data signals using the spread data vector.

51. The method of claim 50 wherein the determined column is a first column of the channel correlation matrix.

52. The method of claim 50 wherein a length of an impulse response of the combined signal is W and the determined column is at least $W - 1$ columns from edges of the channel correlation matrix.

53. The method of claim 50 wherein the determining the spread data vector uses a fourier transform of a hermetian of a channel response matrix multiplied by the received combined signal.

54. The method of claim 50 wherein the determining the spread data vector uses a fourier transform of the determined column.

55. The method of claim 54 wherein the determined column fourier transform is multiplied by a number of spread chips transmitted in the data signals.

56. The method of claim 50 wherein the fourier transform is a fast fourier transform.

57. The method of claim 56 wherein the spread data vector determining further uses an inverse fast fourier transform.

58. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the combined signal;

means for estimating a channel response for the combined signal at the multiple of the chip rate;

means for determining a column of a channel correlation matrix using the estimated channel response;

means for determining a spread data vector using the determined column, the estimated channel response, the received combined signal and a fourier transform; and

means for estimating data of the data signals using the spread data vector.

59. The receiver of claim 58 wherein the determined column is a first column of the channel correlation matrix.

60. The receiver of claim 58 wherein a length of an impulse response of the combined signal is W and the determined column is at least $W - 1$ columns from edges of the channel correlation matrix.

61. The receiver of claim 58 wherein the determining the spread data vector uses a fourier transform of a hermetian of a channel response matrix multiplied by the received combined signal.

62. The receiver of claim 58 wherein the determining the spread data vector uses a fourier transform of the determined column.

63. The receiver of claim 62 wherein the determined column fourier transform is multiplied by a number of spread chips transmitted in the data signals.

64. The receiver of claim 58 wherein the fourier transform is a fast fourier transform.

65. The receiver of claim 58 wherein the spread data vector determining further uses an inverse fast fourier transform.

66. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response for the combined signal at the multiple of the chip rate; and

a single user detection device for determining a column of a channel correlation matrix using the estimated channel response, and for determining a spread data vector using the determined column, the estimated channel response, the received combined signal and a fourier transform; and

wherein data of the data signals is estimated from the spread data vector.

67. The receiver of claim 66 wherein the determined column is a first column of the channel correlation matrix.

68. The method of claim 66 wherein a length of an impulse response of the combined signal is W and the determined column is at least $W - 1$ columns from edges of the channel correlation matrix.

69. The receiver of claim 66 wherein the determining the spread data vector uses a fourier transform of a hermetian of a channel response matrix multiplied by the received combined signal.

70. The receiver of claim 66 wherein the determining the spread data vector uses a fourier transform of the determined column.

71. The receiver of claim 70 wherein the determined column fourier transform is multiplied by a number of spread chips transmitted in the data signals.

72. The receiver of claim 66 wherein the fourier transform is a fast fourier transform.

73. The receiver of claim 66 wherein the spread data vector determining

further uses an inverse fast fourier transform.

74. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the data signals;

combining the multiple chip rate samples as effective chip rate samples;

estimating a channel response for the combined signal at the multiple of the chip rate;

combining the multiple chip rate estimated channel response as an effective chip rate channel response;

determining a spread data vector using the effective samples, the effective channel response and a fourier transform; and

estimating data of the data signals using the spread data vector.

75. The method of claim 74 wherein the multiple chip rate samples and the multiple chip rate estimated channel response are weighted prior to combining.

76. The method of claim 74 wherein the effective chip rate channel response is an effective channel response matrix.

77. The method of claim 74 wherein the determining of the spread data vector uses a column of a channel response matrix derived using the effective chip rate response.

78. The method of claim 74 wherein the column is a first column of the channel response matrix.

79. The method of claim 74 wherein the spread data vector determining further uses an inverse fourier transform.

80. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the data signals;

means for combining the multiple chip rate samples as effective chip rate samples;

means for estimating a channel response for the combined signal at the multiple of the chip rate;

means for combining the multiple chip rate estimated channel response as an effective chip rate channel response;

means for determining a spread data vector using the effective samples, the effective channel response and a fourier transform; and

means for estimating data of the data signals using the spread data vector.

81. The receiver of claim 80 wherein the multiple chip rate samples and the multiple chip rate estimated channel response are weighted prior to combining.

82. The receiver of claim 80 wherein the effective chip rate channel response

is an effective channel response matrix.

83. The receiver of claim 80 wherein the determining of the spread data vector uses a column of a channel response matrix derived using the effective chip rate response.

84. The receiver of claim 80 wherein the column is a first column of the channel response matrix.

85. The receiver of claim 80 wherein the spread data vector determining further uses an inverse fourier transform.

86. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response for the combined signal at the multiple of the chip rate; and

a single user detection device for combining the multiple chip rate samples as effective chip rate samples, for combining the multiple chip rate channel response as an effective chip rate channel response, and for determining a spread data vector using the effective samples, the effective channel response and a fourier transform; and

wherein data of the data signals is estimated from the spread data vector.

87. The receiver of claim 86 wherein the multiple chip rate samples and the multiple chip rate estimated channel response are weighted prior to combining.

88. The receiver of claim 86 wherein the effective chip rate channel response is an effective channel response matrix.

89. The receiver of claim 86 wherein the determining of the spread data vector uses a column of a channel response matrix derived using the effective chip rate response.

90. The receiver of claim 86 wherein the column is a first column of the channel response matrix.

91. The receiver of claim 86 wherein the spread data vector determining further uses an inverse fourier transform.

92. A method for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum in a code division multiple access communication system, each transmitted data signal experiencing a similar channel response, the method comprising:

receiving a combined signal of the transmitted data signals over the shared spectrum;

sampling the combined signal at a multiple of a chip rate of the data signals;

estimating a channel response as a channel response matrix for the combined signal at the multiple of the chip rate;

determining a padded version of a spread data vector of a size corresponding to the multiple chip rate using a column of the channel response matrix, the estimated channel response matrix, the samples and a fourier transform;

estimating the spread data vector by eliminating elements of the padded version so that the estimated spread data vector is of a size corresponding to the chip rate.

93. The method of claim 92 wherein the multiple of the chip rate is an N-multiple of the chip rate and the estimated spread data vector comprises elements of the padded version spaced by N elements.

94. The method of claim 93 further comprising determining an expanded version of the channel response matrix by adding N - 1 columns for every column of the channel response matrix.

95. The method of claim 92 wherein the fourier transform is a fast fourier transform.

96. The method of claim 95 wherein the padded version determining further uses an inverse fast fourier transform.

97. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

means for receiving a combined signal of the transmitted data signals over the shared spectrum;

means for sampling the combined signal at a multiple of a chip rate of the data signals;

means for estimating a channel response as a channel response matrix for the combined signal at the multiple of the chip rate;

means for determining a padded version of a spread data vector of a size

corresponding to the multiple chip rate using a column of the channel response matrix, the estimated channel response matrix, the samples and a fourier transform;

means for estimating the spread data vector by eliminating elements of the padded version so that the estimated spread data vector is of a size corresponding to the chip rate.

98. The receiver of claim 97 wherein the multiple of the chip rate is an N-multiple of the chip rate and the estimated spread data vector comprises elements of the padded version spaced by N elements.

99. The receiver of claim 98 further comprising determining an expanded version of the channel response matrix by adding N - 1 columns for every column of the channel response matrix.

100. The receiver of claim 96 wherein the fourier transform is a fast fourier transform.

101. The receiver of claim 100 wherein the padded version determining further uses an inverse fast fourier transform.

102. A code division multiple access receiver for use in receiving a plurality of data signals transmitted from a transmitter site over a shared spectrum, each transmitted data signal experiencing a similar channel response, the receiver comprising:

an antenna for receiving a combined signal of the transmitted data signals over the shared spectrum;

a sampling device for sampling the combined signal at a multiple of a chip rate of the transmitted data signals;

a channel estimation device for estimating a channel response as a channel response matrix for the combined signal at the multiple of the chip rate;

a single user detection device for determining a padded version of a spread data vector of a size corresponding to the multiple chip rate using a column of the channel response matrix, the estimated channel response matrix, the samples and a fourier transform, and for estimating the spread data vector by eliminating elements of the padded version so that the estimated spread data vector is a size corresponding to the chip rate.

103. The receiver of claim 100 wherein the multiple of the chip rate is an N-multiple of the chip rate and the estimated spread data vector comprises elements of the padded version spaced by N elements.

104. The receiver of claim 101 further comprising determining an expanded version of the channel response matrix by adding N - 1 columns for every column of the channel response matrix.

105. The receiver of claim 102 wherein the fourier transform is a fast fourier transform.

106. The receiver of claim 102 wherein the padded version determining further uses an inverse fast fourier transform.

1/8

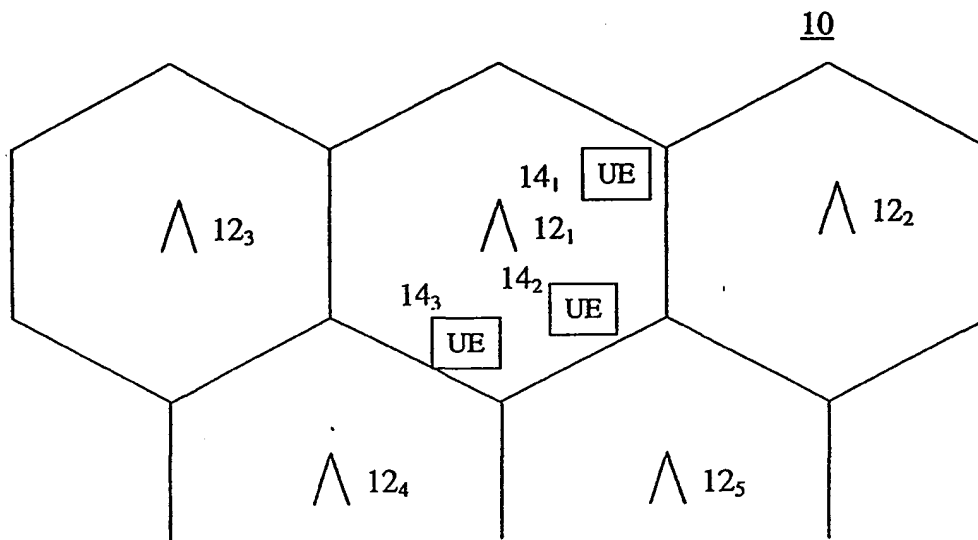


FIG. 1

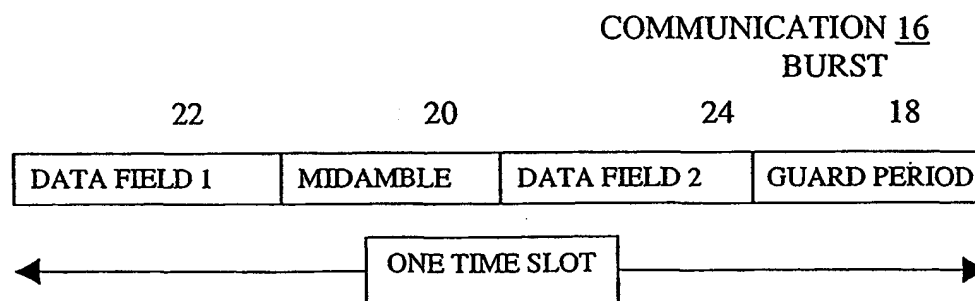


FIG. 3

2/8

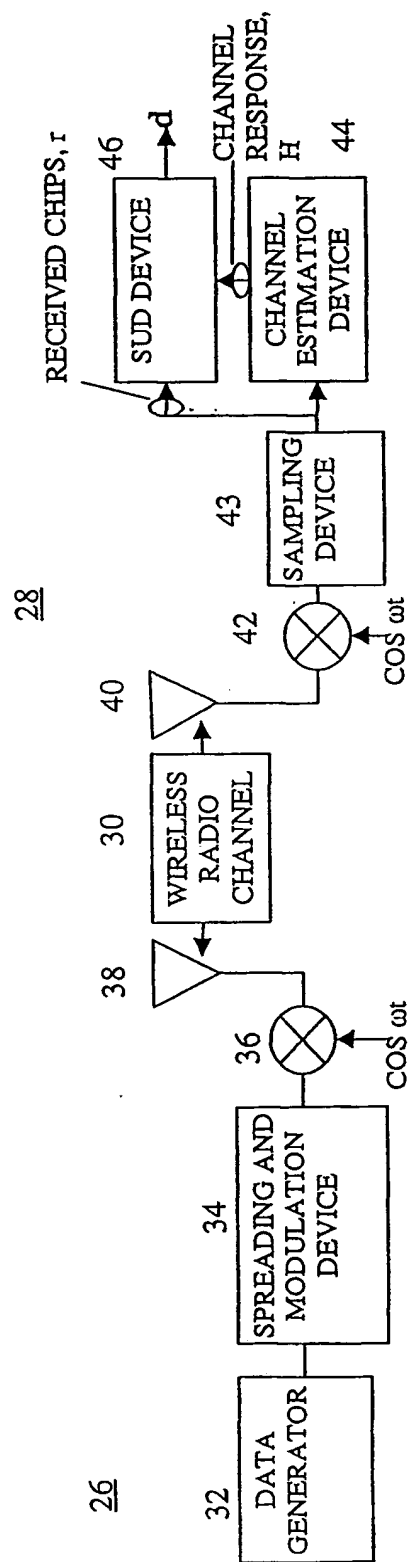


Fig. 2

3/8

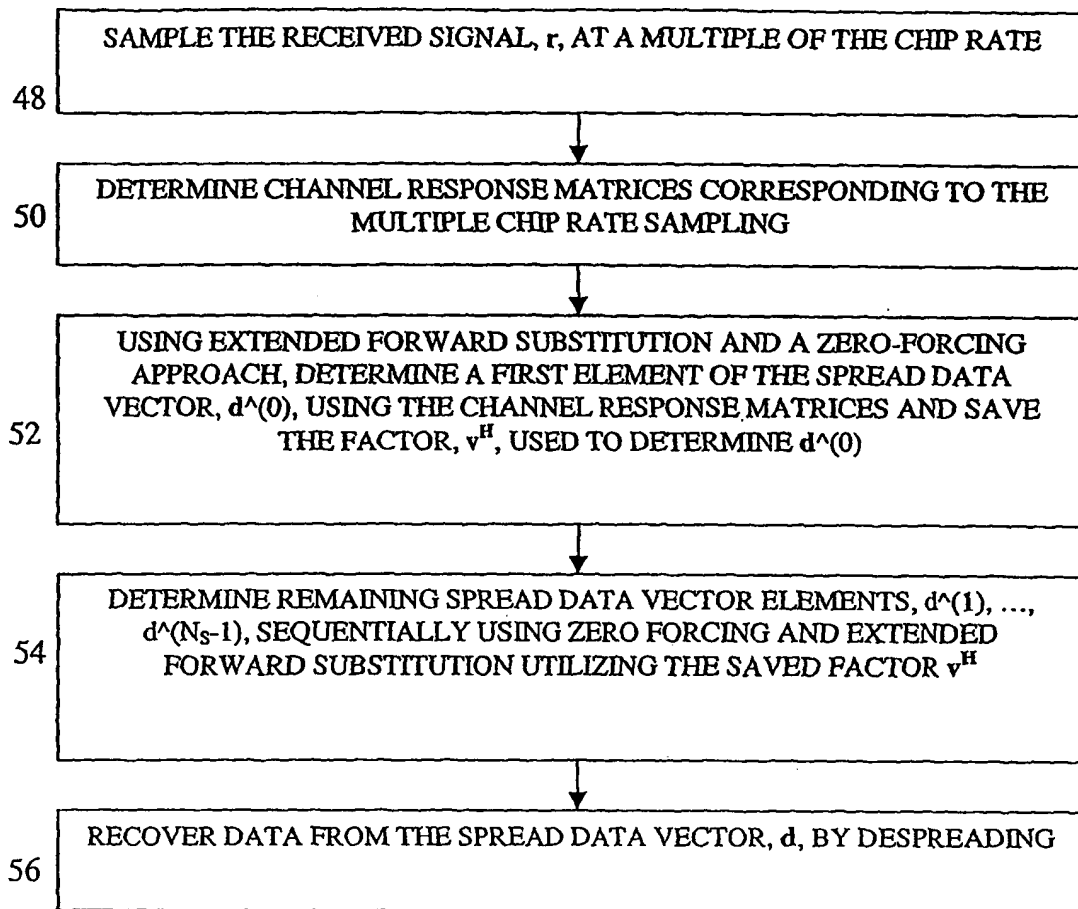


FIG. 4

4/8

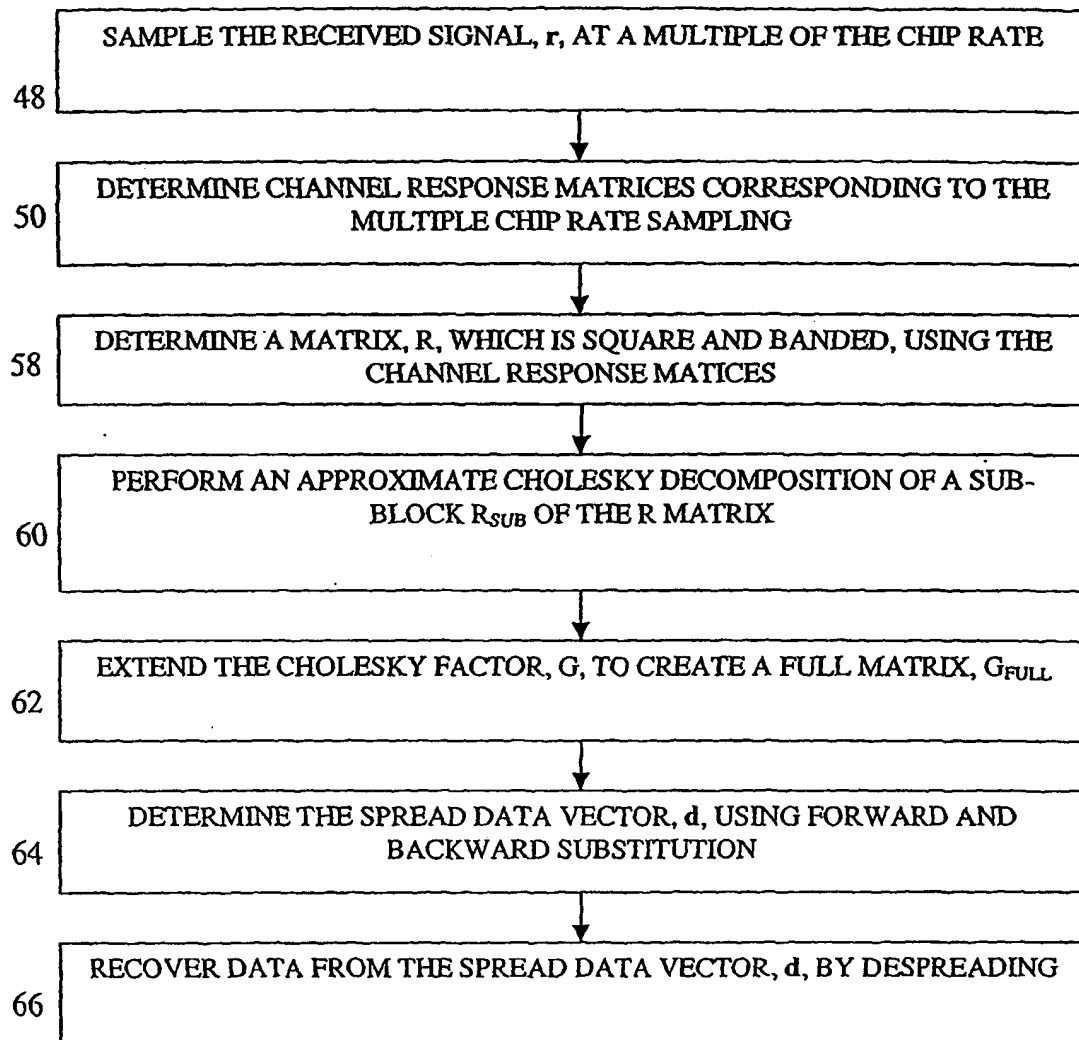


FIG. 5

5/8

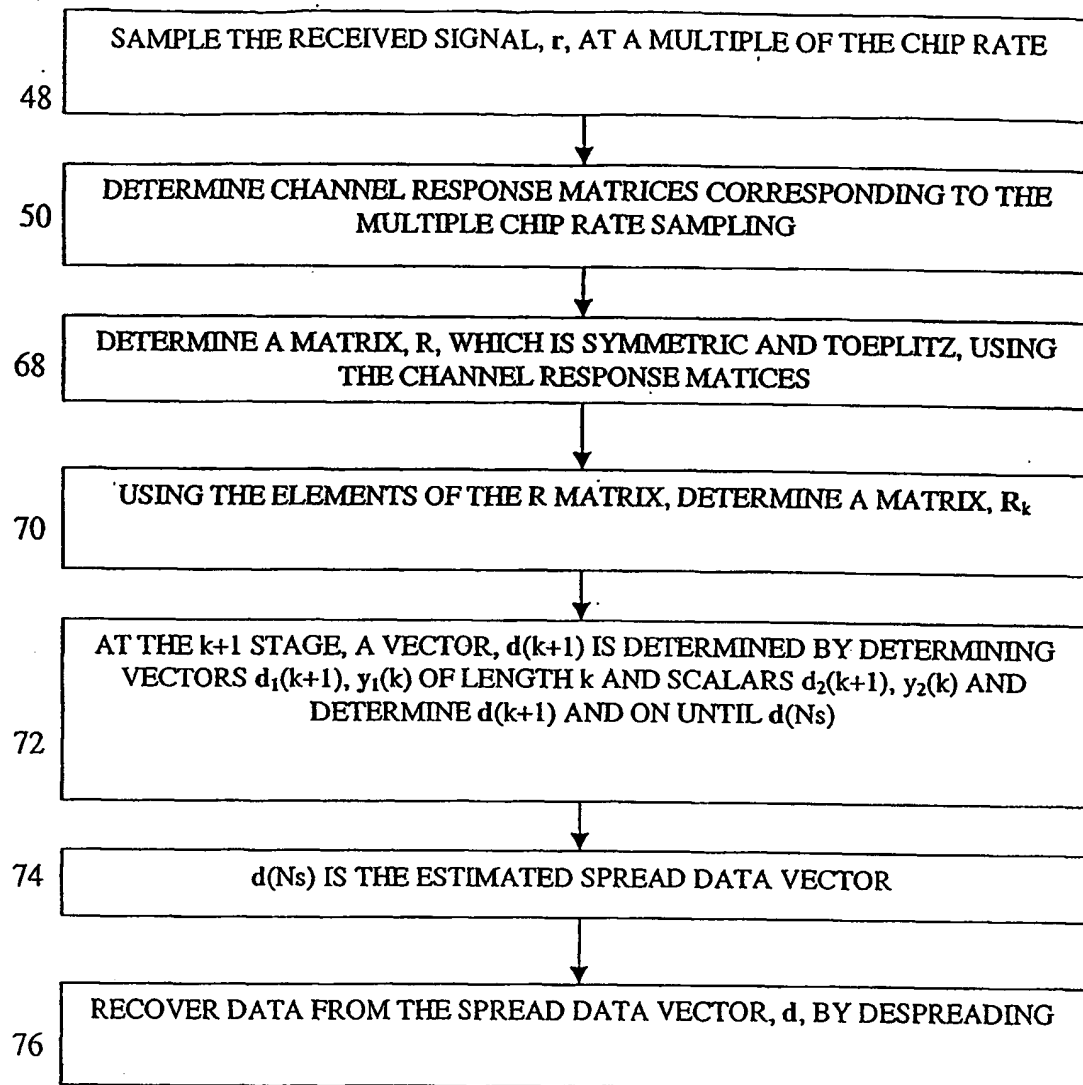


FIG. 6

6/8

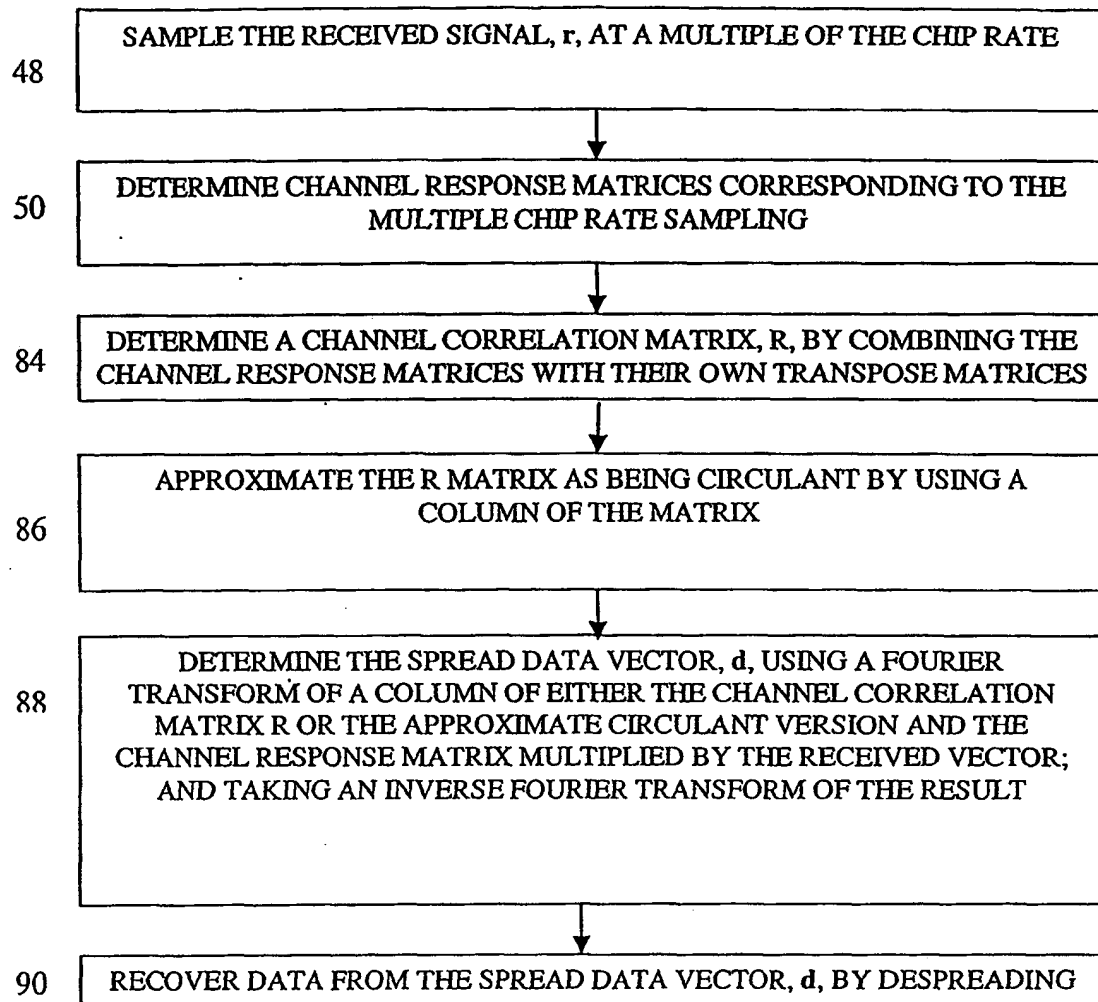


FIG. 7

7/8

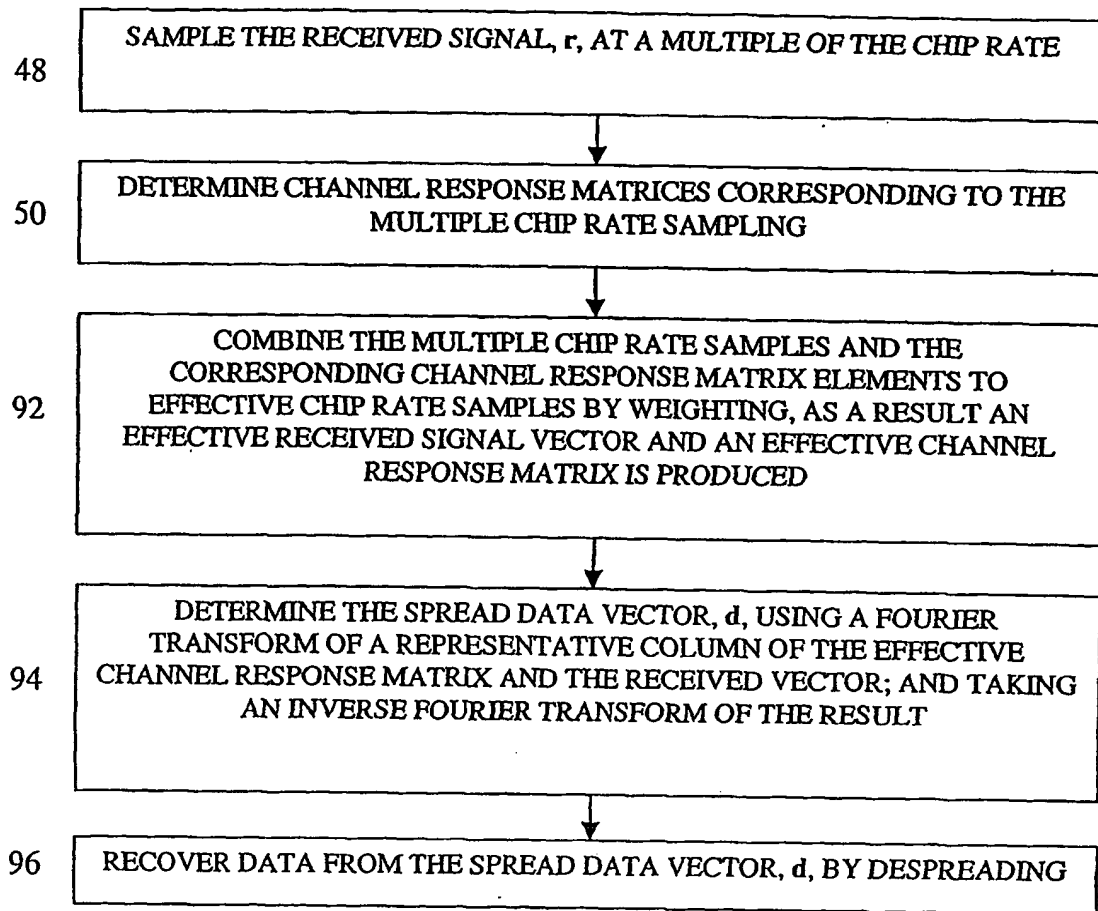


FIG. 8

8/8

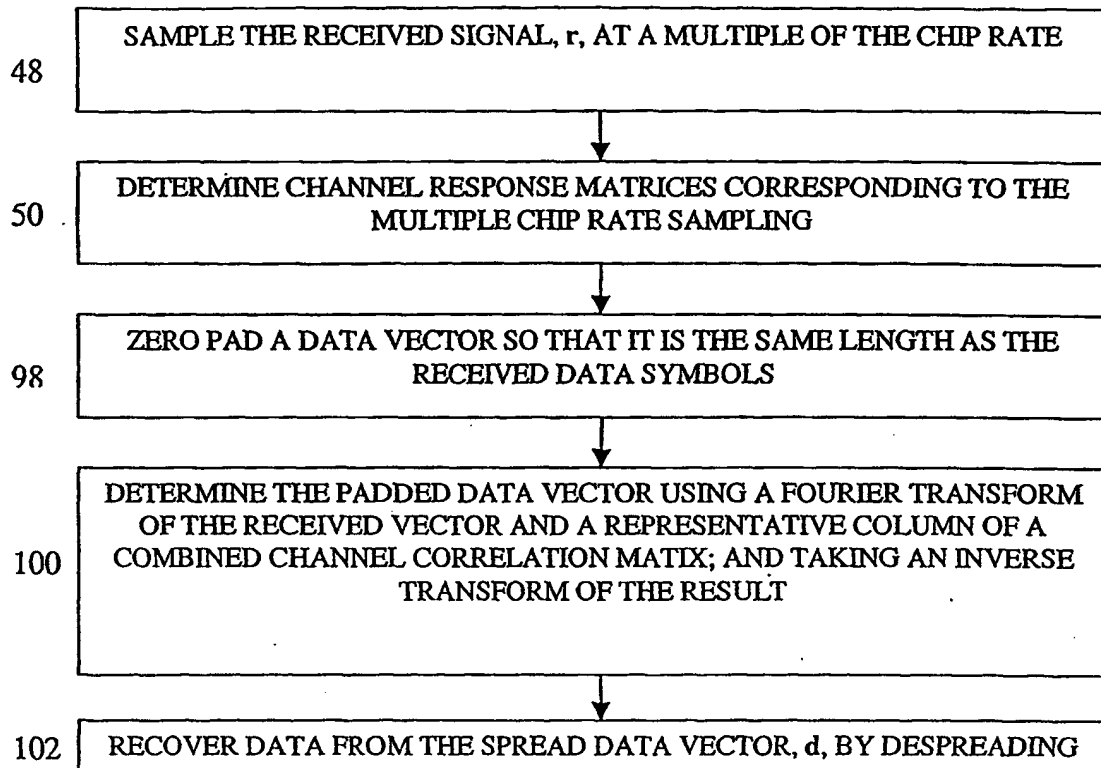


FIG. 9